2

Noise and Propagation mechanisms

Noise

Johnson-Nyquist noise

Physical review 1928

$V_{rms}^2 = 4kTBR$

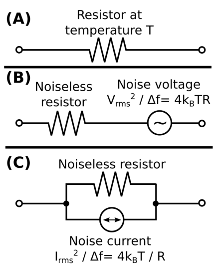
k : Bolzmann's constant

T : absolute temperature

B : bandwidth

R : Resistance

P=4kTB



Why is this a simplification?

$V_{rms}^2 = 4kTBR$

B -> infinity => P -> infinity

Correction:

Replace kT with $h/(e^{hf/kT}-1)$

h : Planck's constant

No effect until we are in the THz range.

(But we are there now for some systems!)

Standard noise temperature

We set a standard temperature of 290 K for noise calculations

290 K = 16.85 C ("Room temperature")

Calculate noise in 1 Hz bandwith:

$P = kTB = 1.38x10^{-23}$ x 290 x 1 = 4 x 10^{-21} W = -174 dBm

(Exact answer -173.975188679)

P = -204 dBW

Noise in 1kHz Bandwidth: -144 dBm

Noise factor and noise figure

Noise figure NF = 10 log (Noise factor F)

$F=N_{out}/kT_0G$

$(S/N)_{out}$ = (S/N)in + NF at 290 K

Cascade formule

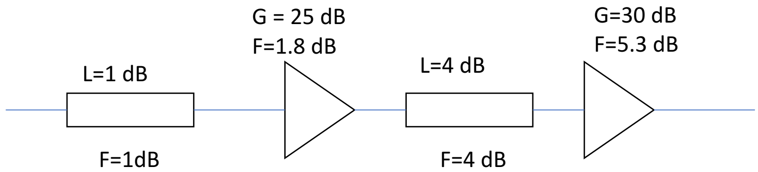
Total noise factor of a system:

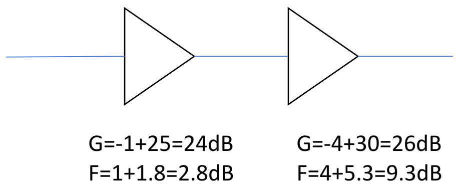
$F_T=F_1 + (F_2-1)/G_1 + (F_3-1)/G_1G_2 + \ldots + (F_N-1)/(G_1G_2\ldots G_{N-1})$

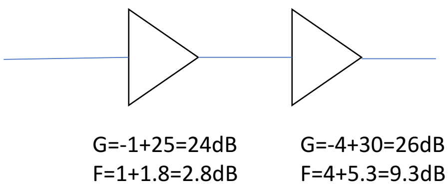
Noise factor of a amplifier: look it up

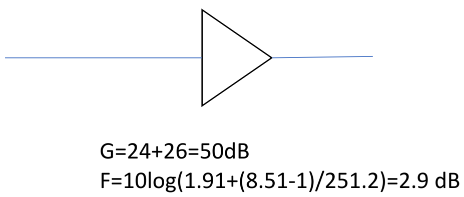
Noise factor of a loss at 290K: L=NF

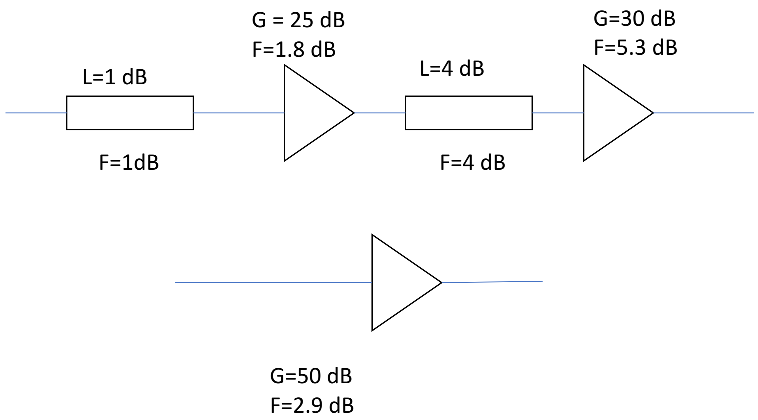
Example


G = 25 dB
F=1.8 dB
G=30 dB
F=5.3 dB
L=1 dB
L=4 dB
F=1dB
F=4 dB


G=-1+25=24dB
F=1+1.8=2.8dB
G=-4+30=26dB
F=4+5.3=9.3dB


G=-1+25=24dB
F=1+1.8=2.8dB
G=-4+30=26dB
F=4+5.3=9.3dB


G=24+26=50dB
F=10log(1.91+(8.51-1)/251.2)=2.9 dB

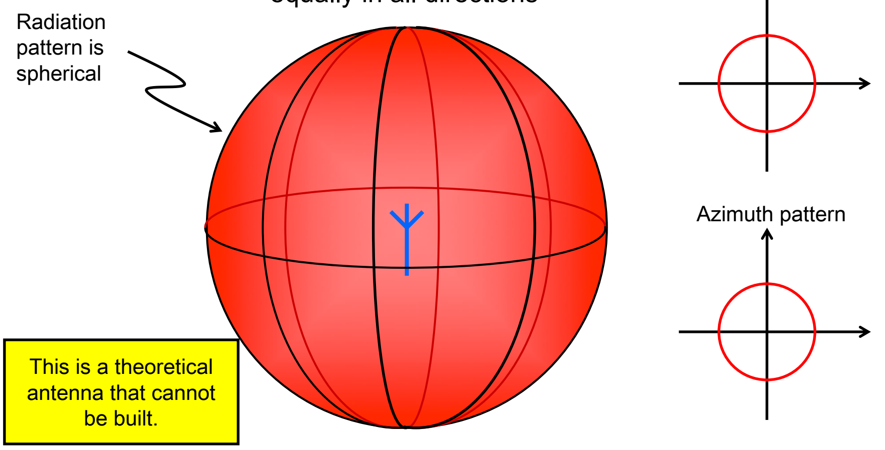


Mini-circuits

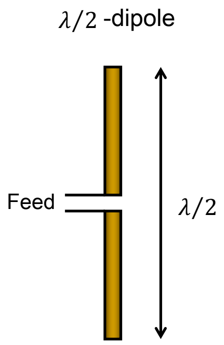
ANTENNA BASICS

The isotropic antenna

The **isotropic antenna** radiates equally in all directions

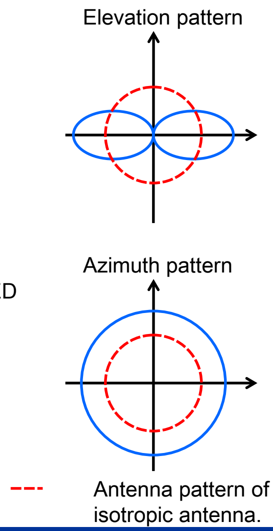


The dipole antenna



This antenna does not radiate straight up or down. Therefore, more energy is available in other directions.

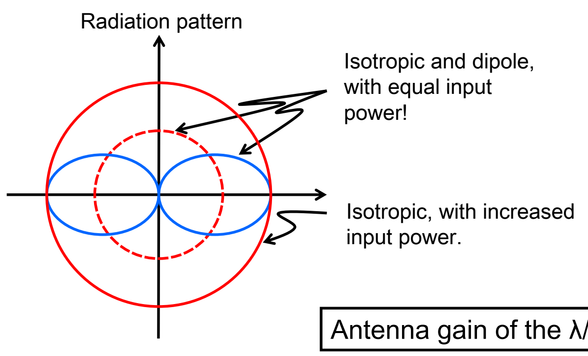
THIS IS THE PRINCIPLE BEHIND WHAT IS CALLED ***ANTENNA GAIN***.



Antenna gain (principle)

Antenna gain is a relative measure.

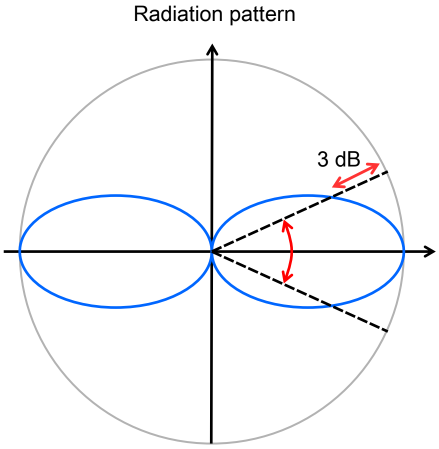
We will use the isotropic antenna as the reference.



The increase of input power to the isotropic antenna, to obtain the same maximum radiation is called the **antenna gain!**

Antenna gain of the $\lambda/2$ dipole is **2.15 dBi**.

Antenna beamwidth (principle)



The isotropic antenna has ”no” beamwidth. It radiates equally in all directions.

The **half-power beamwidth** is measured between points were the pattern as decreased by 3 dB.

Receiving antennas

In terms of gain and beamwidth, an antenna has the same properties when used as transmitting or receiving antenna.

A useful property of a receiving antenna is its ”**effective area**”, i.e. the area from which the antenna can ”absorb” the power from an incoming electromagnetic wave.

Effective area A_{RX} of an antenna is connected to its gain:

$$G_{RX} = \frac{A_{RX}}{A_{ISO}} = \frac{4\pi}{\lambda^2} A_{RX}$$

It can be shown that the effectiva are of the isotropic antenna is:

$$A_{ISO} = \frac{\lambda^2}{4\pi}$$

Note that A_{ISO} becomes smaller with increasing frequency, i.e. with smaller wavelength.

A note on antenna gain

Sometimes the notation **dBi** is used for antenna gain (instead of dB).

The ”i” indicates that it is the gain relative to the isotropic antenna (which we will use in this course).

Another measure of antenna gain frequently encountered is **dBd**, which is relative to the λ/2 dipole.

$$G|_{dBi} = G|_{dBd} + 2.15\ dB$$

Be careful! Sometimes it is not clear if the antenna gain is given in dBi or dBd.

EIRP
Effective Isotropic Radiated Power

EIRP = Transmit power (fed to the antenna) + antenna gain

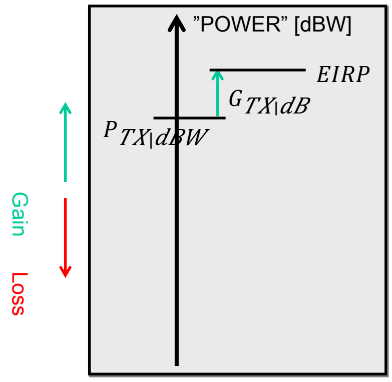
$$EIRP|_{dBW} = P_{TX|dBW} + G_{TX|dB}$$

Answers the questions:

How much transmit power would we need to feed an isotropic antenna to obtain the same maximum on the radiated power?

How ”strong” is our radiation in the maximal direction of the antenna?

EIRP and the link budget



$$EIRP|_{dBW} = P_{TX|dBW} + G_{TX|dB}$$

PROPAGATION MECHANISMS

Propagation mechanisms

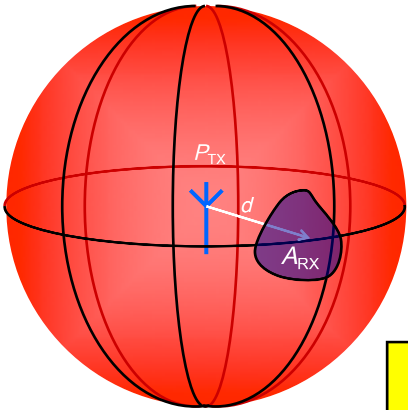
•We are going to study the fundamental propagation mechanisms

•This has two purposes:
–Gain an understanding of the basic mechanisms
–Derive propagation losses that we can use in calculations

•For many of the mechanisms, we just give a brief overview

FREE SPACE PROPAGATION

Free-space loss
Derivation



If we assume RX antenna to be isotropic:

$$P_{RX} = \frac{\lambda^2/4\pi}{4\pi d^2} P_{TX} = \left(\frac{\lambda}{4\pi d}\right)^2 P_{TX}$$

Assumptions:

Isotropic TX antenna

TX power P_{TX}

Distance d

RX antenna with effective area A_{RX}

Relations:

Area of sphere: $A_{tot} = 4\pi d^2$

Received power: $P_{RX} = \frac{A_{RX}}{A_{tot}} P_{TX}$

$= \frac{A_{RX}}{4\pi d^2} P_{TX}$

Attenuation between two isotropic antennas in free space is (free-space loss):

$$L_{free}(d) = \left(\frac{4\pi d}{\lambda}\right)^2$$

Free-space loss
Non-isotropic antennas

Received power, with isotropic antennas (G_{TX}=G_{RX}=1):

$$P_{RX}(d) = \frac{P_{TX}}{L_{free}(d)}$$

Received power, with antenna gains G_{TX} and G_{RX}:

$$P_{RX}(d) = \frac{G_{RX} G_{TX}}{L_{free}(d)} P_{TX} \Leftrightarrow P_{RX|dBW}(d) = P_{TX|dBW} + G_{TX|dB} - L_{free|dB}(d) + G_{R}$$

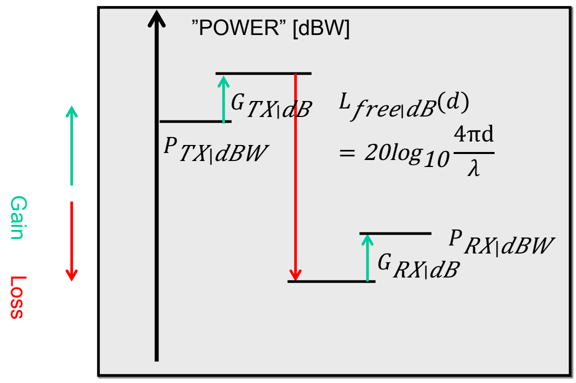
$$= P_{TX|dBW} + G_{TX|dB} - 20\log_{10}\left(\frac{4\pi d}{\lambda}\right) + G_{RX|dB}$$

$$= \frac{G_{RX} G_{TX}}{\left(\frac{4\pi d}{\lambda}\right)^2} P_{TX}$$

This relation is called **Friis' law**

Free-space loss
Non-isotropic antennas (cont.)

Let's put Friis' law into the link budget



Received power decreases as $1/d^2$, which means a **propagation exponent** of $n = 2$.

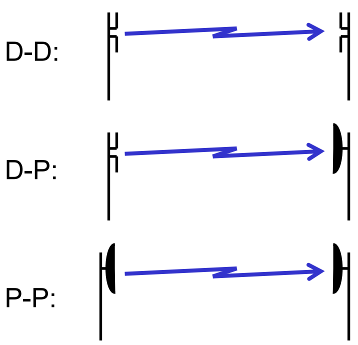
How come that the received power decreases with increasing frequency (decreasing λ)?

Does it?

$$P_{RX|dBW}(d) = P_{TX|dBW} + G_{TX|dB} - L_{free|dB}(d) + G_{RX|dB}$$

Free-space loss
Example: Antenna gains

Assume following three free-space scenarios with λ/2 dipoles and parabolic antennas with fixed effective area A_{par}:



Antenna gains

$$G_{dip|dB} = 2.15 \text{ dBi}$$

$$G_{par|dB} = 10\log_{10}\frac{A_{par}}{A_{iso}} = 10\log_{10}\frac{A_{par}}{\lambda^2/4\pi} = 10\log_{10}\frac{4\pi A_{par}}{\lambda^2}$$

Free-space loss
Example: Antenna gains (cont.)

Evaluation of Friis' law for the three scenarios:

D-D:

$$P_{RX|dBW}(d) = P_{TX|dBW} + 2.15 - 20log_{10}\left(\frac{4\pi d}{\lambda}\right) + 2.15$$
$$= P_{TX|dBW} + 4.3 - 20log_{10}(4\pi d) + 20log_{10}\lambda$$

Received power decreases with decreasing wavelength λ, i.e. with increasing frequency.

D-P:

$$P_{RX|dBW}(d) = P_{TX|dBW} + 2.15 - 20log_{10}\left(\frac{4\pi d}{\lambda}\right) + 10log_{10}\left(\frac{4\pi A_{par}}{\lambda^2}\right)$$
$$= P_{TX|dBW} + 2.15 - 20log_{10}(4\pi d) + 10log_{10}(4\pi A_{par})$$

Received power independent of wavelength, i.e. of frequency.

P-P:

$$P_{RX|dBW}(d) = P_{TX|dBW} + 10log_{10}\left(\frac{4\pi A_{par}}{\lambda^2}\right) - 20log_{10}\left(\frac{4\pi d}{\lambda}\right) + 10log_{10}\left(\frac{4\pi A_{par}}{\lambda^2}\right)$$
$$= P_{TX|dBW} + 20log_{10}(4\pi A_{par}) - 20log_{10}(4\pi d) - 20log_{10}\lambda$$

Received power increases with decreasing wavelength λ, i.e. with increasing frequency.

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Free-space loss
Validity - the Rayleigh distance

The free-space loss calculations are only valid in the **far field** of the antennas.

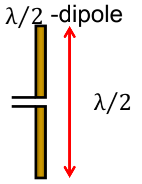
Far-field conditions are assumed "**far beyond"** the Rayleigh distance:

$$d_R = 2\frac{{L_a}^2}{\lambda}$$

where L_a is the largest dimesion of the antenna.

Another rule of thumb is:
"**At least** N wavelengths"

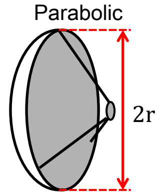
λ/2 -dipole



$L_a = \lambda/2$

$d_R = \lambda/2$

Parabolic



$L_a = 2r$

$d_R = \frac{8r^2}{\lambda}$

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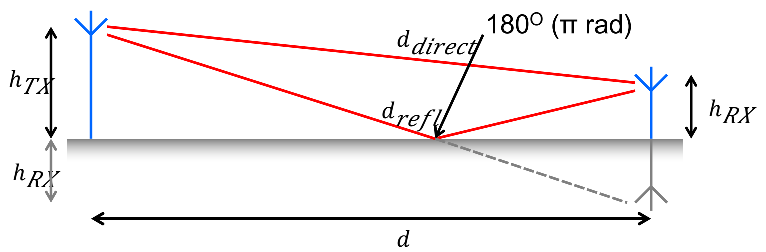
PROPAGATION OVER A GROUND PLANE

Propagation over ground plane Geometry



Propagation distances:

$$d_{direct} = \sqrt{d^2 + \left(h_{TX} - h_{RX}\right)^2}$$

$$d_{refl} = \sqrt{d^2 + \left(h_{TX} + h_{RX}\right)^2}$$

$$\Delta d = d_{refl} - d_{direct}$$

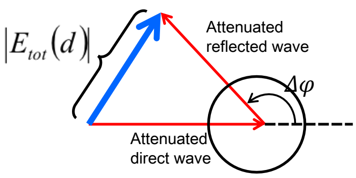
Phase difference at RX antenna:

$$\Delta\varphi = 2\pi\frac{\Delta d}{\lambda} + \pi = 2\pi\left(f\frac{\Delta d}{c} + \frac{1}{2}\right)$$

Propagation over ground plane Geometry

What happens when the two waves are combined?

Vector addition of electric fields



Taking the free-space propagation losses into account for each wave, the exact expression becomes rather complicated.

Assuming equal free-space attenuation on the two waves we get:

$$|E_{tot}(d)| = |E(d)| \times |1 + e^{j\Delta\varphi}|$$

Free space attenuated — Extra attenuation

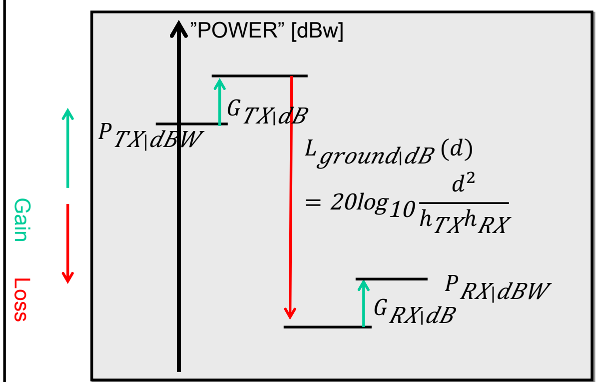
Finally, after applying an approximation of the phase difference:

$$L_{ground}(d) \approx \left(\frac{4\pi d}{\lambda}\right)^2 \left(\frac{\lambda d}{4\pi h_{TX} h_{RX}}\right)^2 = \frac{d^4}{h_{TX}^2 h_{RX}^2}$$

Approximation valid when: $d \geq d_{limit} = \frac{4 h_{TX} h_{RX}}{\lambda}$

Propagation over ground plane Non-isotropic antennas

Let's put L_{ground} into the link budget

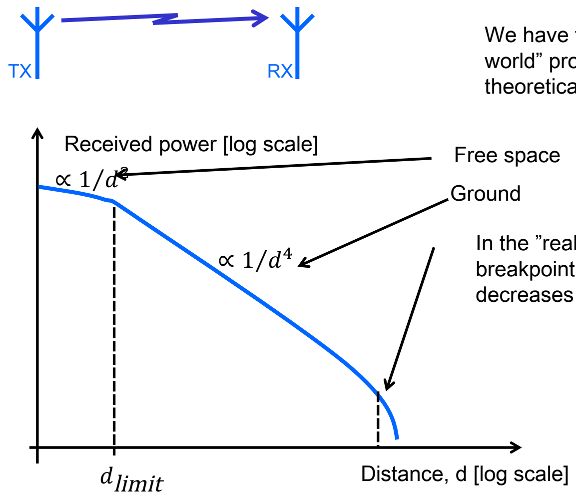


Received power decreases as $1/d^4$, which means a **propagation exponent** of $n = 4$.

There is no frequency dependence on the propagation attenuation, which was the case for free space.

$$P_{RX|dBW}(d) = P_{TX|dBW} + G_{TX|dB} - L_{ground|dB}(d) + G_{RX|dB}$$

Rough comparison to ”real world”

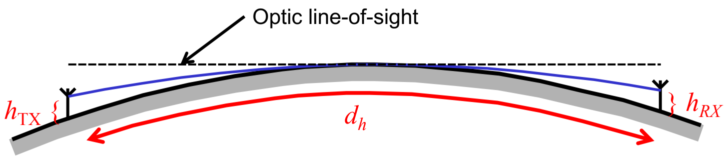


We have tried to explain ”real world” propagation loss using theoretical models.

In the ”real world” there is one more breakpoint, where the received power decreases much faster than $1/d^4$.

Rough comparison to ”real world” (cont.)

One thing that we have not taken into account: **Curvature of earth**!

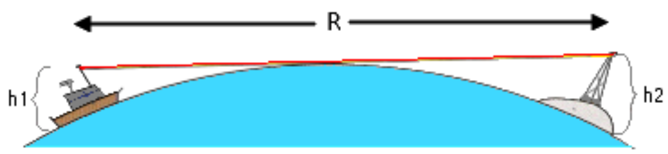


An approximation of the radio horizon:

$$d_h \approx 4.1 \left(\sqrt{h_{TX|m}} + \sqrt{h_{RX|m}} \right)|_{km}$$

beyond which received power decays very rapidly.

Nautic application



$R = 2.2(\sqrt{h1} + \sqrt{h2})$

R here in nautical miles, 1 NM = 1,852 km

Example: Voyager 2

Distance: 1.7×10^{13} m

Uplink

Frequency: 2 115 MHz

Power: 20 kW = 73 dBm

Downlink

Frequency 2 295 MHz / 8 415 MHz

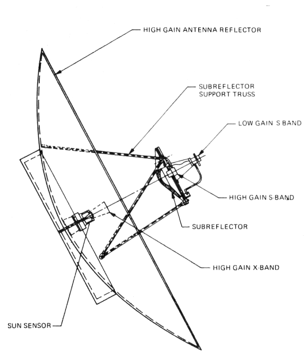
Power: 22 W = 43 dBm

Antenna gains

$$Gain\ (dB) = 10 \times \log_{10} k \left(\frac{\pi D}{\lambda}\right)^2$$

Ground antenna: 70 m parabolic dish
Gain: 63.8 dB (62.1 dB)
(Rayleigh distance: 69 137 m)

Sattelite antenna: 3.7 m parabolic dish
Gain: 49.5 dB (35 dB)
(Rayleigh distance: 193 m)



Path Loss

$$L_{free}(d) = \left(\frac{4\pi d}{\lambda}\right)^2$$

d = 1.7x10^{13} m
Lambda = c / f = 3x10^{8} / 2 115 x 10^{6} = 0.14 m

PL = 2.33x10^{30} = 304 dB

Noise

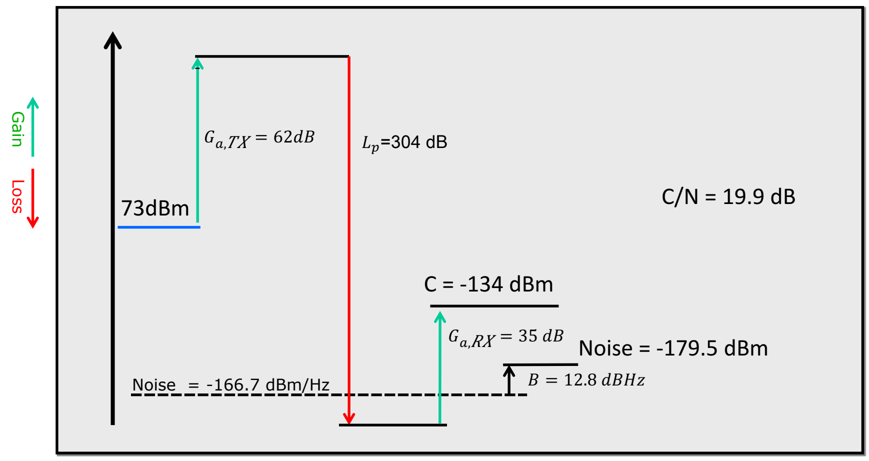
Bandwidth = 12.8 dB-Hz = 19 Hz

Noise density at reciever :

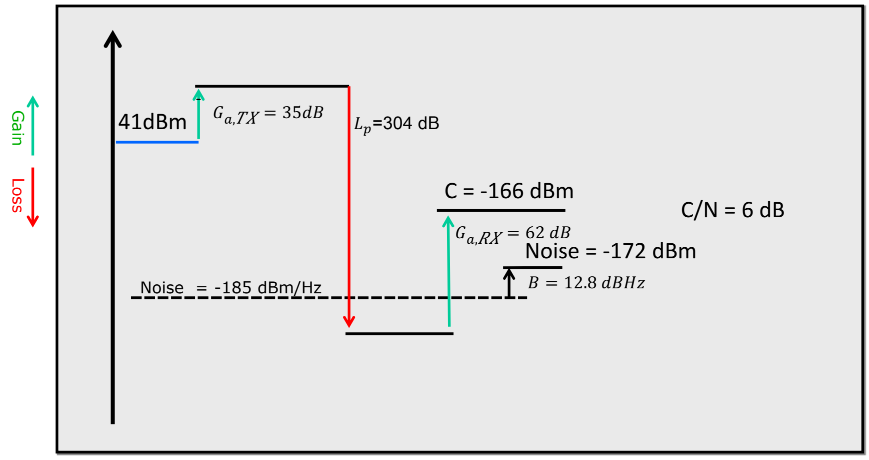
Satellite: -167 dBm/Hz

Ground: -185 dBm/Hz

Voyager link budget Uplink (v.1)

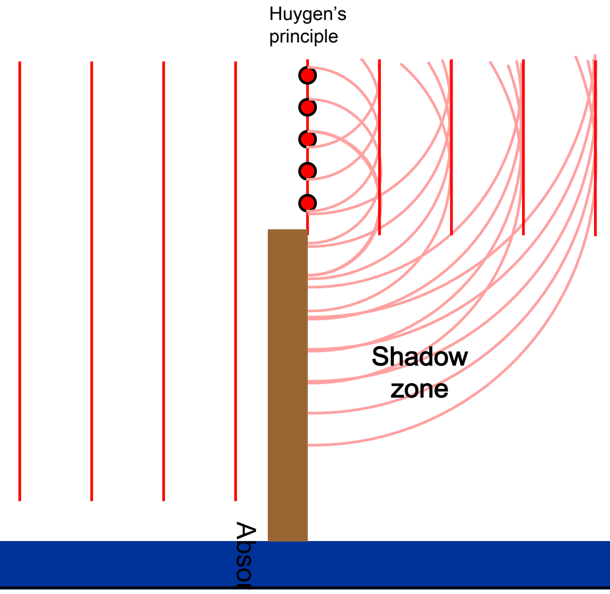


Voyager link budget Downlink (v.1)



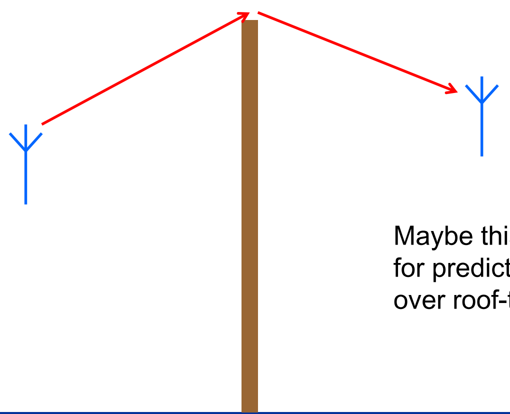
DIFFRACTION

Diffraction
Absorbing screen



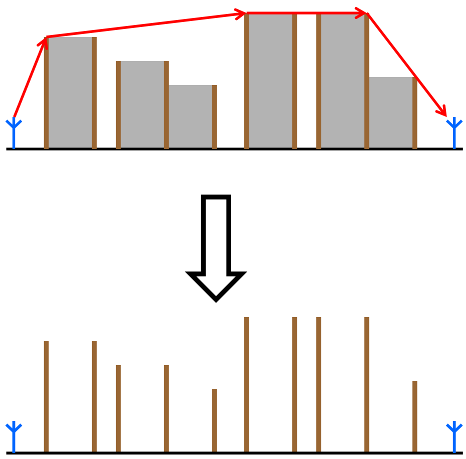
Diffraction
Absorbing screen (cont.)

For the case of one screen we have exact solutions or good approximations



Maybe this is a good solution for predicting propagation over roof-tops?

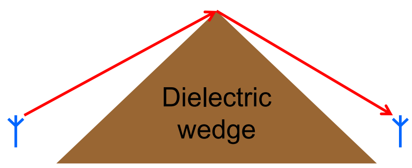
Diffraction
Approximating buildnings



There are no solutions for multiple screens, except for very special cases!

Several approximations of varying quality exist.
[See textbook]

Diffraction
Wedges

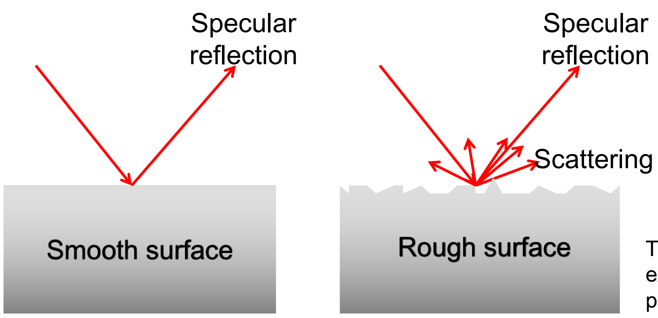


Reasonably simple far-field approximations exist.

Can be used to model terrain or obstacles

SCATTERING BY ROUGH SURFACES

Scattering by rough surfaces Scattering mechanism



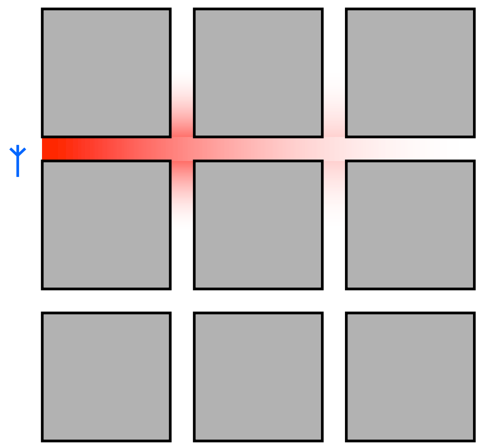
Due to the ”roughness” of the surface, some of the power of the specular reflection lost and is scattered in other directions.

Two main theories exist: Kirchhoff and pertubation.

Both rely on statistical descriptions of the surface height.

WAVEGUIDING

Waveguiding
Street canyons, corridors & tunnels



Conventional waveguide theory predicts exponential loss with distance.

The waveguides in a radio environment are different:

- Lossy materials
- Not continuous walls
- Rough surfaces
- Filled with metallic and dielectric obstacles

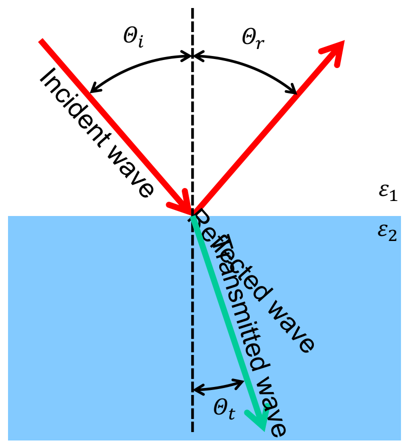
Majority of measurements fit the $1/d^n$ law.

Summary

- Some **dB** calculations
- Antenna **gain** and **effective area**.
- Propagation in **free space**, **Friis' law** and **Rayleigh distance**.
- Propagation over a **ground plane**.
- Diffraction
- Screens
- Wedges
- Multiple screens
- Scattering by rough surfaces
- Waveguiding

REFLECTION AND TRANSMISSION

Reflection and transmission
Snell's law



ε_1 Dielectric
ε_2 constants

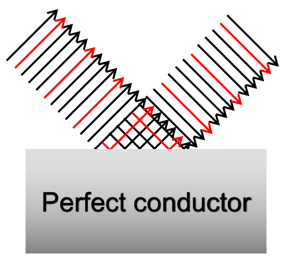
$$\begin{cases} \Theta_i = \Theta_r \\ \dfrac{\sin\Theta_t}{\sin\Theta_i} = \dfrac{\sqrt{\varepsilon_1}}{\sqrt{\varepsilon_2}} \end{cases}$$

Reflection and transmission
Refl./transm. coefficcients

Given complex dielectric constants of the materials, we can also compute the reflection and transmission coefficients for incoming waves of different polarization.

[See textbook.]

The property we are going to use:



No loss and the electric field is phase shifted 180^{O} (changes sign).